



# MP2174C

## 2.7V-5.5V, 4A, High-Efficiency, Synchronous Step-Down Converter with Forced CCM in 2×2mm QFN

### DESCRIPTION

The MP2174C is a monolithic, step-down, switch mode converter with built-in, internal power MOSFETs. It achieves 4A of continuous output current from a 2.7V to 5.5V input voltage with excellent load and line regulation. The output voltage can be regulated as low as 0.6V.

The constant-on-time (COT) control scheme provides fast transient response and easy loop stabilization.

Fault condition protections include cycle-by-cycle current limit and thermal shutdown.

The MP2174C requires a minimal number of readily available, standard external components, and is available in an ultra-small QFN-12 (2mmx2mm) package.

The MP2174C is ideal for a wide range of applications, including PDAs, portable instruments, DVD drives, and small handheld devices.

### FEATURES

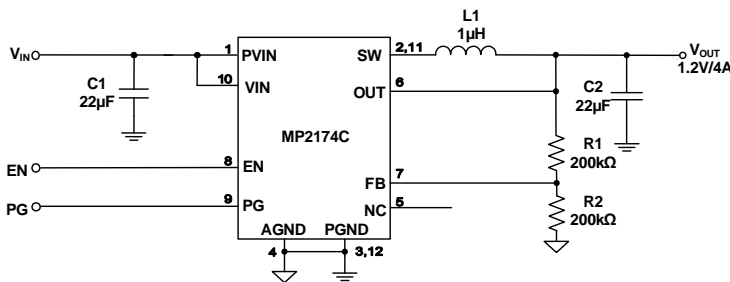
- Forced PWM Mode Operation
- Wide 2.7V to 5.5V Operating Input Range
- Output Voltage as Low as 0.6V
- 4A Output Current
- 35mΩ and 18mΩ Internal Power MOSFET
- Peak Efficiency Above 96%
- 1.1MHz Frequency
- 100% Duty Cycle in Dropout
- 0.5ms Internal Soft-Start Time
- EN and Power Good for Power Sequencing
- Auto-Discharge at Power-Off
- Short-Circuit Protection with Hiccup Mode
- Available in a QFN-12 (2mmx2mm) Package

### APPLICATIONS

- Storage Drives
- Portable/Handheld Devices
- Low-Voltage I/O System Power

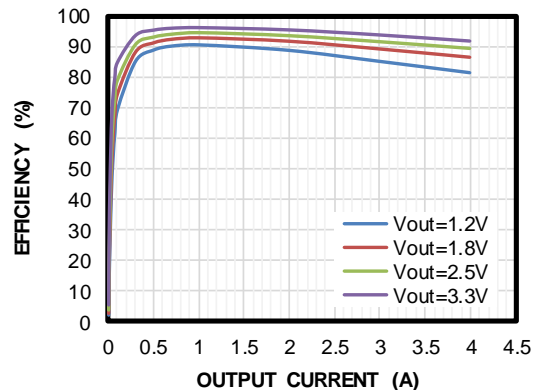
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### TYPICAL APPLICATION



### Efficiency vs. Output Current

V<sub>IN</sub> = 5V, DCR = 27mΩ



## ORDERING INFORMATION

Part Number*	Package	Top Marking
MP2174CGG	QFN12 (2mm x 2mm)	See Below

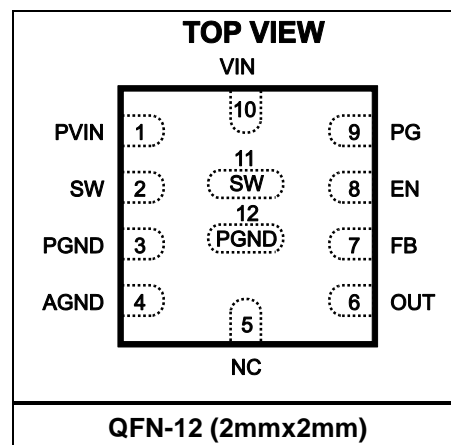
\* For Tape & Reel, add suffix –Z (e.g. MP2174CGG–Z).

## TOP MARKING

\_\_\_\_\_  
**KCY**  
**LLL**

KC: Product code of MP2174CGG  
 Y: Year code  
 LLL: Lot number

## PACKAGE REFERENCE



## PIN FUNCTIONS

Pin #	Name	Description
1	PVIN	<b>Supply voltage to power FETs.</b> PVIN is connected to VIN internally.
2, 11	SW	<b>Switch output.</b> Pin 2 and 11 can be connected together.
3, 12	PGND	<b>Power ground.</b> Pin 3 and 12 can be connected together.
4	AGND	<b>Quiet ground for controller circuits.</b>
5	NC	<b>No connection.</b> Leave this pin open. Do not connect it to ground.
6	OUT	<b>Input sense pin for output voltage.</b>
7	FB	<b>Feedback.</b> An external resistor divider from the output to GND, tapped to the FB pin, sets the output voltage.
8	EN	<b>On/off control.</b>
9	PG	<b>Power good indicator.</b> The output of this pin is an open drain pin.
10	VIN	<b>Supply voltage to internal control circuitry.</b> VIN is connected to PVIN internally.

**ABSOLUTE MAXIMUM RATINGS** <sup>(1)</sup>

Supply voltage ( $V_{IN}$ ) .....	6.5V
$V_{SW}$ .....	
-0.3V (-3V for <10ns) to +6.5V (8V for <10ns)	
All other pins .....	-0.3V to +6.5V
Junction temperature .....	150°C
Lead temperature .....	260°C
Continuous power dissipation ( $T_A = 25^\circ\text{C}$ ) <sup>(2)</sup>	
.....	1.6W
Storage temperature.....	-65°C to +150°C

**Recommended Operating Conditions** <sup>(3)</sup>

Supply voltage ( $V_{IN}$ ) .....	2.7V to 5.5V
Operating junction temp ( $T_J$ ) ....	-40°C to +125°C

<b>Thermal Resistance</b>	$\theta_{JA}$	$\theta_{JC}$
QFN-12 (2mmx2mm)		
EV2174C-G-00A <sup>(4)</sup> .....	45.....	8....°C/W
JESD51-7 <sup>(5)</sup> .....	80.....	16...°C/W

**Notes:**

- 1) Exceeding these ratings may damage the device.
- 2) The maximum allowable power dissipation is a function of the maximum junction temperature  $T_J$  (MAX), the junction-to-ambient thermal resistance  $\theta_{JA}$ , and the ambient temperature  $T_A$ . The maximum allowable continuous power dissipation at any ambient temperature is calculated by  $P_D$  (MAX) =  $(T_J$  (MAX) -  $T_A$ ) /  $\theta_{JA}$ . Exceeding the maximum allowable power dissipation will cause excessive die temperature, and the regulator will go into thermal shutdown. Internal thermal shutdown circuitry protects the device from permanent damage.
- 3) The device is not guaranteed to function outside of its operating conditions.
- 4) Measured on EV2174C-G-00A, 2-layer PCB, 63mmx63mm.
- 5) Measured on JESD51-7, 4-layer PCB. The value of  $\theta_{JA}$  given in this table is only valid for comparison with other packages and cannot be used for design purposes. These values are calculated in accordance with JESD51-7, and simulated on a specified JEDEC board. They do not represent the performance obtained in an actual application.

## ELECTRICAL CHARACTERISTICS

$V_{IN} = 3.6V$ ,  $T_A = -40^{\circ}C$  to  $+125^{\circ}C$  <sup>(6)</sup>, typical value is tested at  $T_J = 25^{\circ}C$ , unless otherwise noted.

Parameter	Symbol	Condition	Min	Typ	Max	Units
Feedback voltage	$V_{FB}$	$2.7V \leq V_{IN} \leq 5.5V$ $T_J = 25^{\circ}C$	594	600	606	mV
Feedback voltage	$V_{FB}$	$2.7V \leq V_{IN} \leq 5.5V$	588	600	612	mV
Feedback current	$I_{FB}$	$V_{FB} = 0.63V$		10	50	nA
PFET switch on resistance	$R_{DSON\_P}$	$V_{IN} = 5V$		35		m $\Omega$
NFET switch on resistance	$R_{DSON\_N}$	$V_{IN} = 5V$		18		m $\Omega$
Switch leakage		$V_{EN} = 0V$ , $V_{IN} = 5.5V$ , $V_{SW} = 0V$ and $5.5V$ , $T_J = 25^{\circ}C$		0	5	$\mu A$
PFET peak current limit <sup>(7)</sup>		$T_J = 25^{\circ}C$	5	6.5		A
NFET valley current limit <sup>(7)</sup>				4.5		A
On time	$t_{ON}$	$V_{IN} = 5V$ , $V_{OUT} = 1.2V$		220		ns
		$V_{IN} = 3.6V$ , $V_{OUT} = 1.2V$		300		
Switching frequency	$f_{SW}$	$V_{OUT} = 1.2V$		1100		kHz
Minimum off time	$t_{MIN-OFF}$			100		ns
Minimum on time <sup>(7)</sup>	$t_{MIN-ON}$			80		ns
Soft-start time	$t_{SS-ON}$	From 10% $V_{OUT}$ to 90% $V_{OUT}$		0.5	1	ms
Soft-stop time	$t_{SS-OFF}$	From 90% $V_{OUT}$ to 10% $V_{OUT}$			0.3	ms
EN off delay		$V_{EN}$ off to 90% $V_{OUT}$ drop			0.4	ms
Power good upper trip threshold		FB with respect to the regulation		+10		%
Power good lower trip threshold				-10		%
Power good delay		Rising		90		$\mu s$
Power good sink current capability	$V_{PG\_LO}$	Sink 1mA			0.4	V
Power good logic high voltage	$V_{PG\_HI}$	$V_{IN} = 5V$ , $V_{FB} = 0.63V$	4.9			V
Under-voltage lockout threshold rising		$-40^{\circ}C \leq T_J \leq +85^{\circ}C$		2.48	2.68	V
Under-voltage lockout threshold hysteresis				450		mV

**ELECTRICAL CHARACTERISTICS (continued)**
 $V_{IN} = 3.6V$ ,  $T_A = -40^{\circ}C$  to  $+125^{\circ}C$  <sup>(6)</sup>, typical value is tested at  $T_J = 25^{\circ}C$ , unless otherwise noted.

Parameter	Symbol	Condition	Min	Typ	Max	Units
EN turn-on delay <sup>(7)</sup>		EN on to SW active		255		$\mu s$
EN rising threshold			0.5	0.65	0.9	V
EN hysteresis				0.09		V
EN input current		$V_{EN} = 2V$		2		$\mu A$
		$V_{EN} = 0V$		0		$\mu A$
Supply current (shutdown)		$V_{EN} = 0V$ , $T_J = 25^{\circ}C$		0	1	$\mu A$
Supply current (quiescent)		$V_{EN} = 2V$ , $V_{FB} = 0.63V$ , $V_{IN} = 3.6V$ , $T_J = 25^{\circ}C$		500		$\mu A$
Thermal shutdown <sup>(7)</sup>				155		$^{\circ}C$
Thermal hysteresis <sup>(7)</sup>				25		$^{\circ}C$

**Notes:**

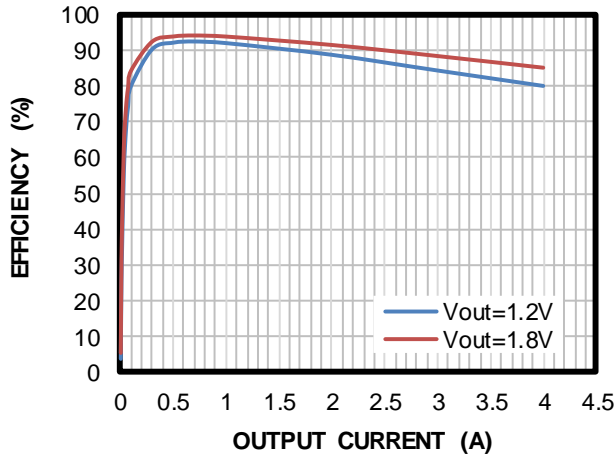
- 6) Not tested in production. Guaranteed by over-temperature correlation.  
 7) Guaranteed by engineering sample characterization.

## TYPICAL PERFORMANCE CHARACTERISTICS

$V_{IN} = 5V$ ,  $V_{OUT} = 1.2V$ ,  $L = 1\mu H$ ,  $T_A = 25^\circ C$ , unless otherwise noted.

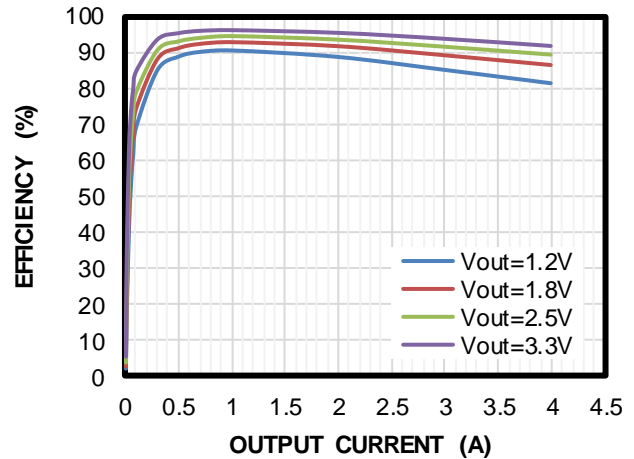
**Efficiency vs. Output Current**

$V_{IN} = 3.3V$



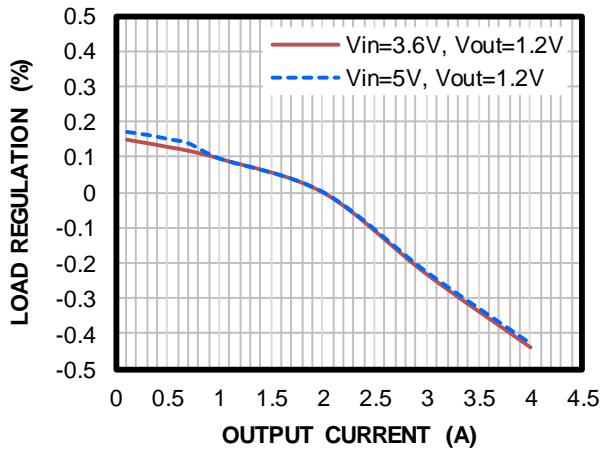
**Efficiency vs. Output Current**

$V_{IN} = 5V$



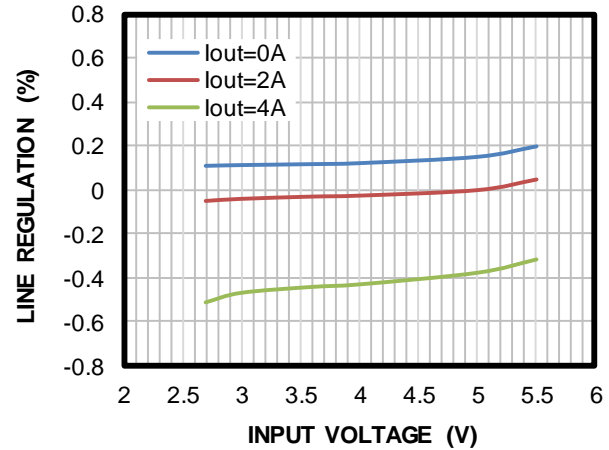
**Load Regulation vs. Output Current**

$V_{IN} = 3.6V/5V$ ,  $I_{OUT} = 0.1A$  to  $4A$

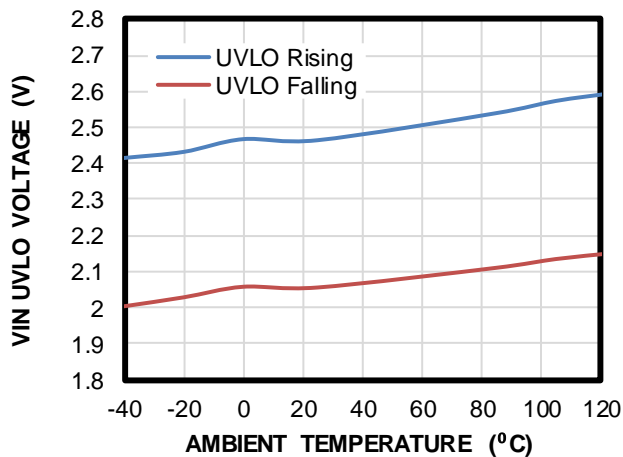


**Line Regulation vs. Output Current**

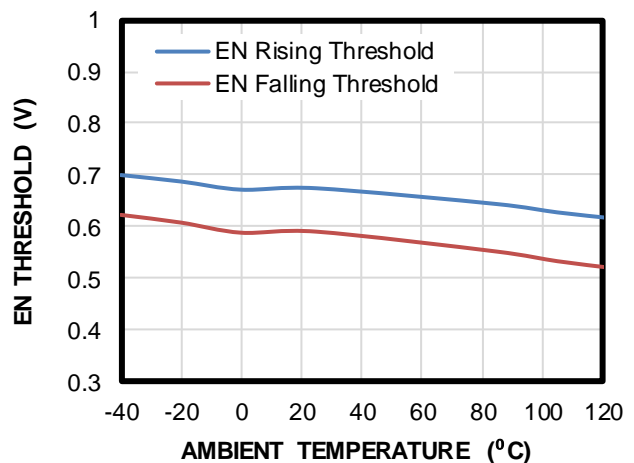
$V_{IN} = 2.7V$  to  $5.5V$



**VIN UVLO vs. Temperature**



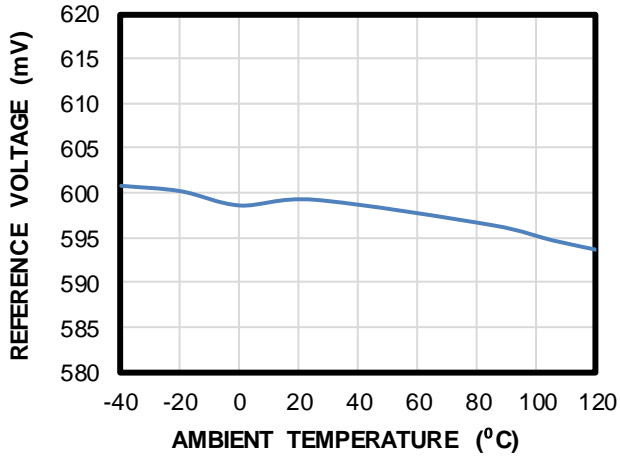
**EN Threshold vs. Temperature**



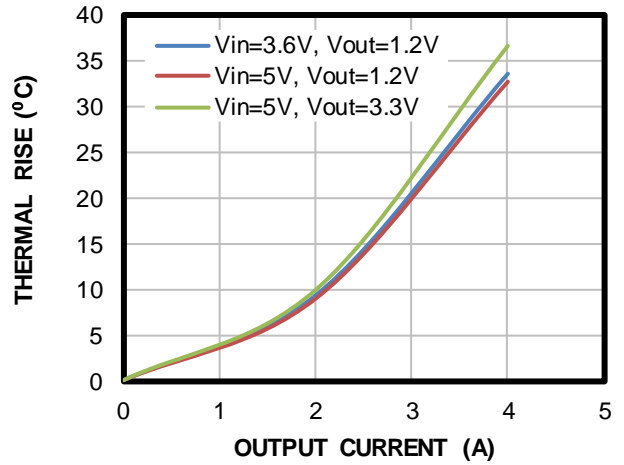
**TYPICAL PERFORMANCE CHARACTERISTICS (continued)**

$V_{IN} = 5V$ ,  $V_{OUT} = 1.2V$ ,  $L = 1\mu H$ ,  $T_A = 25^\circ C$ , unless otherwise noted.

**Reference Voltage vs. Temperature**



**Thermal Rise vs. Output Current**

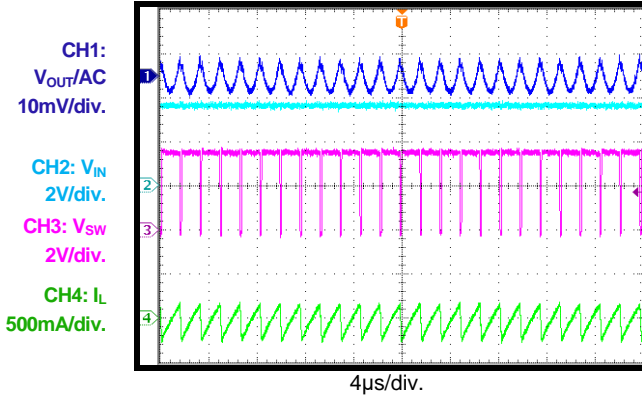


**TYPICAL PERFORMANCE CHARACTERISTICS (continued)**

$V_{IN} = 5V$ ,  $V_{OUT} = 1.2V$ ,  $L = 1\mu H$ ,  $T_A = 25^\circ C$ , unless otherwise noted.

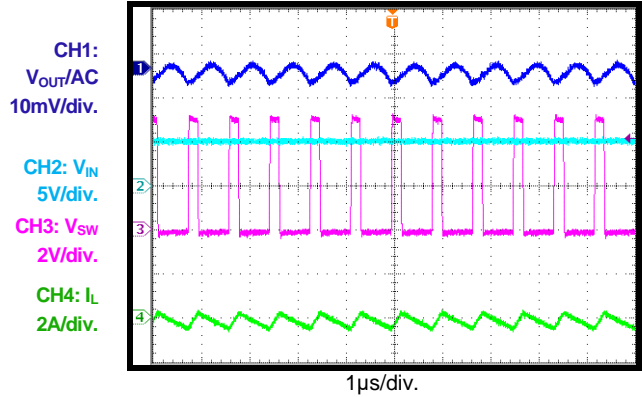
**Output Ripple**

$V_{IN} = 3.6V$ ,  $V_{OUT} = 3.3V$ ,  $I_{OUT} = 0A$



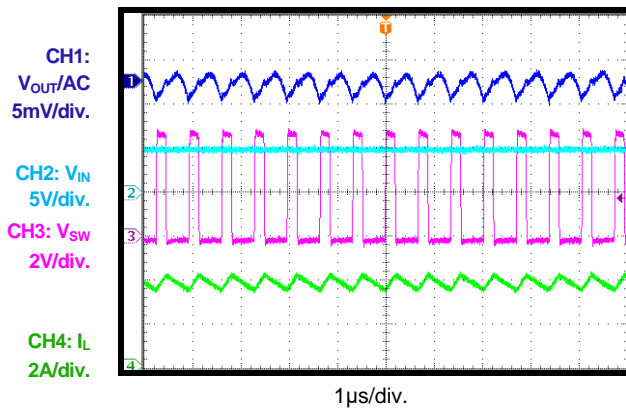
**Output Ripple**

$V_{IN} = 5V$ ,  $V_{OUT} = 1.2V$ ,  $I_{OUT} = 0A$



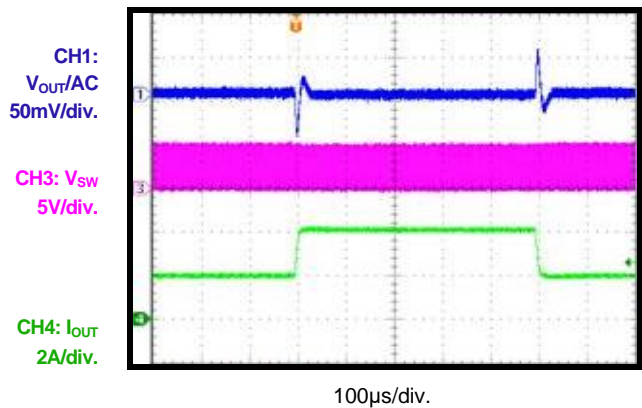
**Output Ripple**

$V_{IN} = 5V$ ,  $V_{OUT} = 1.2V$ ,  $I_{OUT} = 4A$



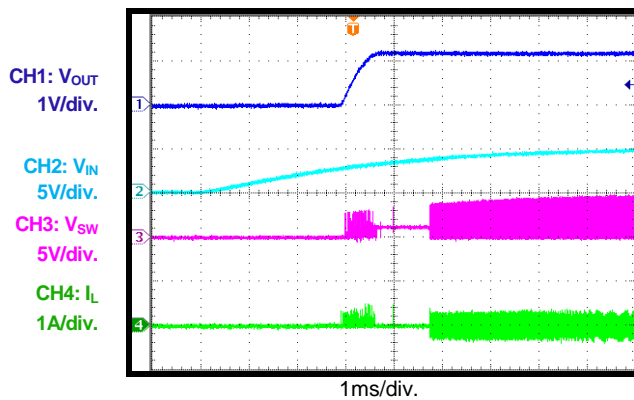
**Transient**

$I_{OUT} = 2A$  to  $4A$ ,  $2.5A/\mu s$



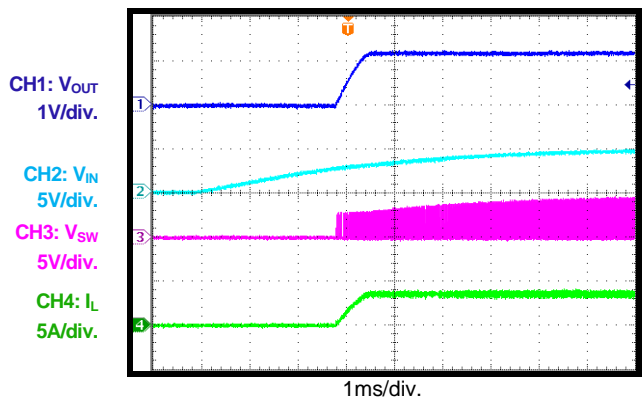
**VIN Start-Up**

$I_{OUT} = 0A$



**VIN Start-Up**

$I_{OUT} = 4A$



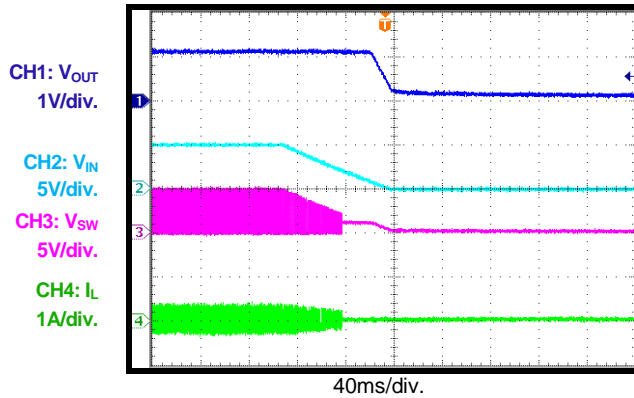


**TYPICAL PERFORMANCE CHARACTERISTICS (continued)**

$V_{IN} = 5V$ ,  $V_{OUT} = 1.2V$ ,  $L = 1\mu H$ ,  $T_A = 25^\circ C$ , unless otherwise noted.

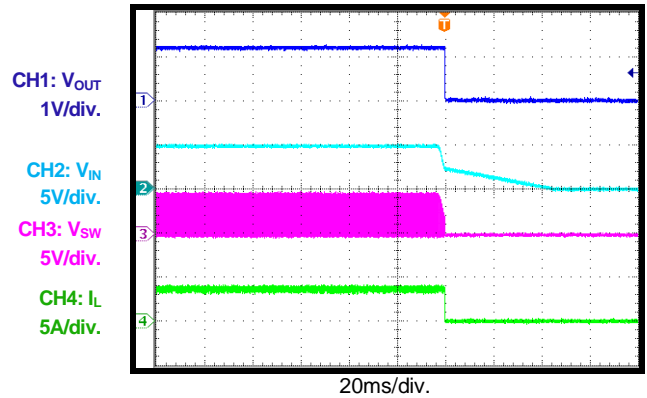
**VIN Shutdown**

$I_{OUT} = 0A$



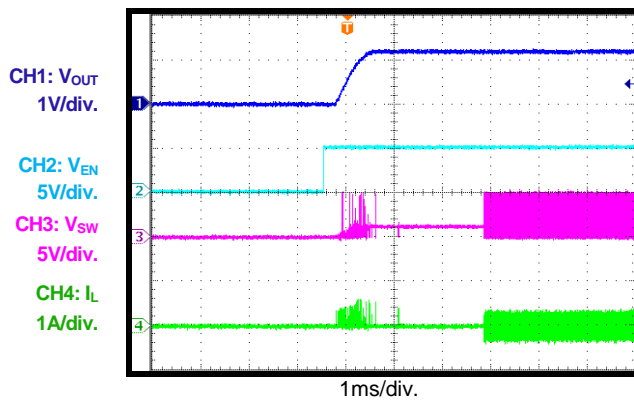
**VIN Shutdown**

$I_{OUT} = 4A$



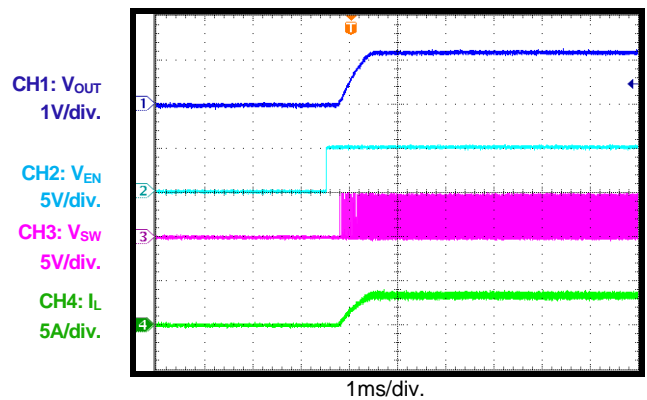
**EN Start-Up**

$I_{OUT} = 0A$



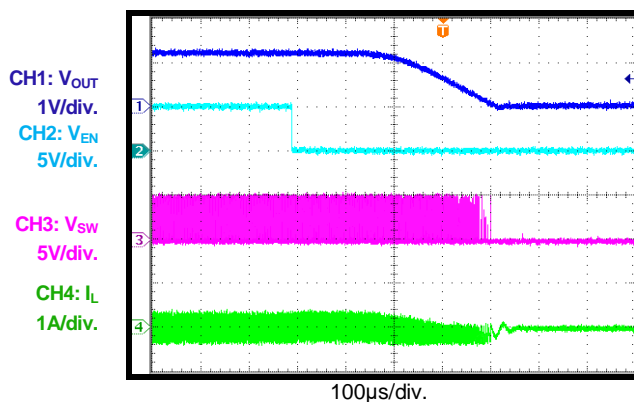
**EN Start-Up**

$I_{OUT} = 4A$



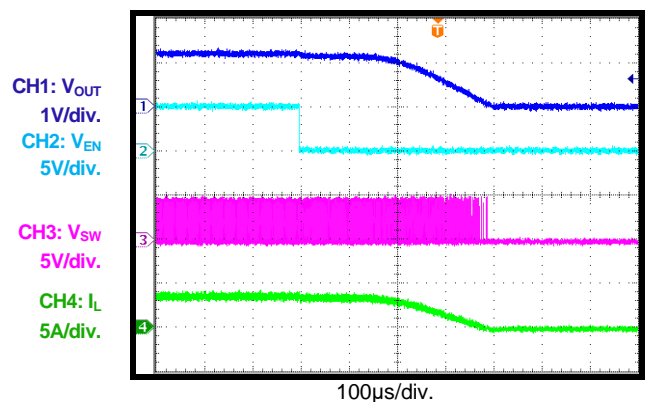
**EN Shutdown**

$I_{OUT} = 0A$



**EN Shutdown**

$I_{OUT} = 4A$

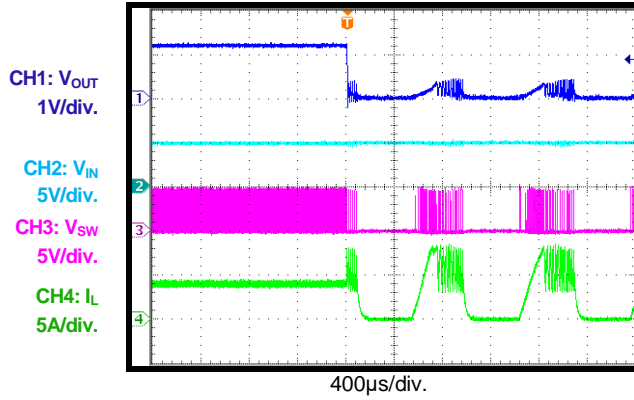


**TYPICAL PERFORMANCE CHARACTERISTICS (continued)**

$V_{IN} = 5V$ ,  $V_{OUT} = 1.2V$ ,  $L = 1\mu H$ ,  $T_A = 25^\circ C$ , unless otherwise noted.

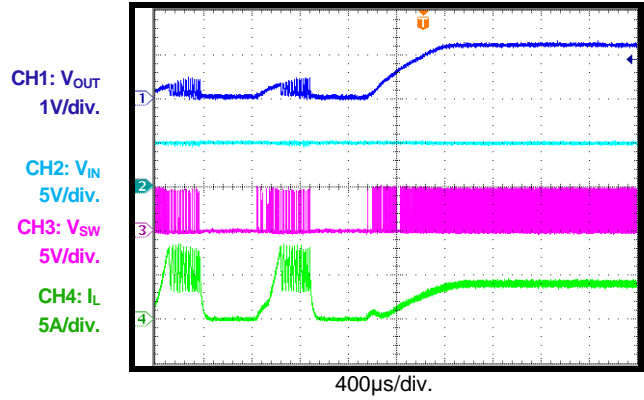
**SCP Entry**

$I_{OUT} = 4A$



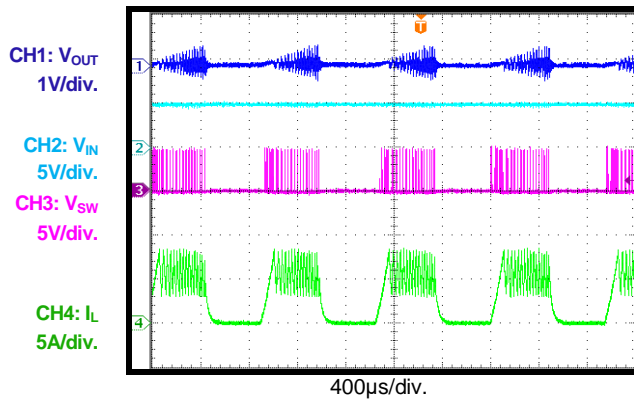
**SCP Recovery**

$I_{OUT} = 4A$



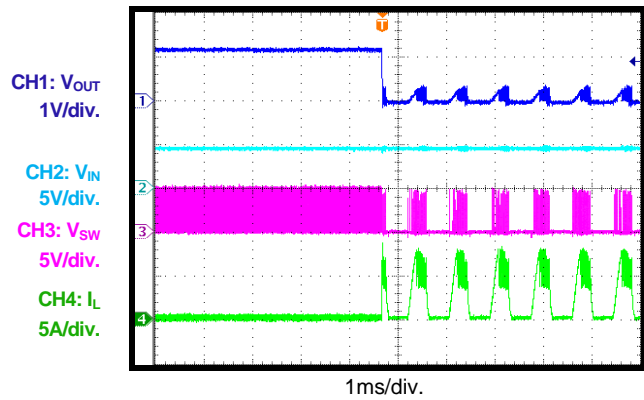
**SCP State**

$I_{OUT} = 4A$



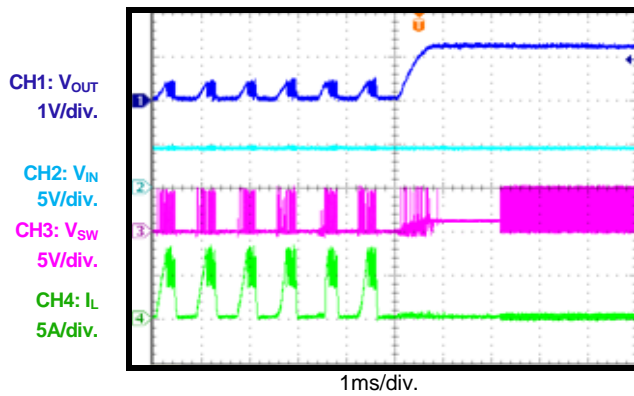
**SCP Entry**

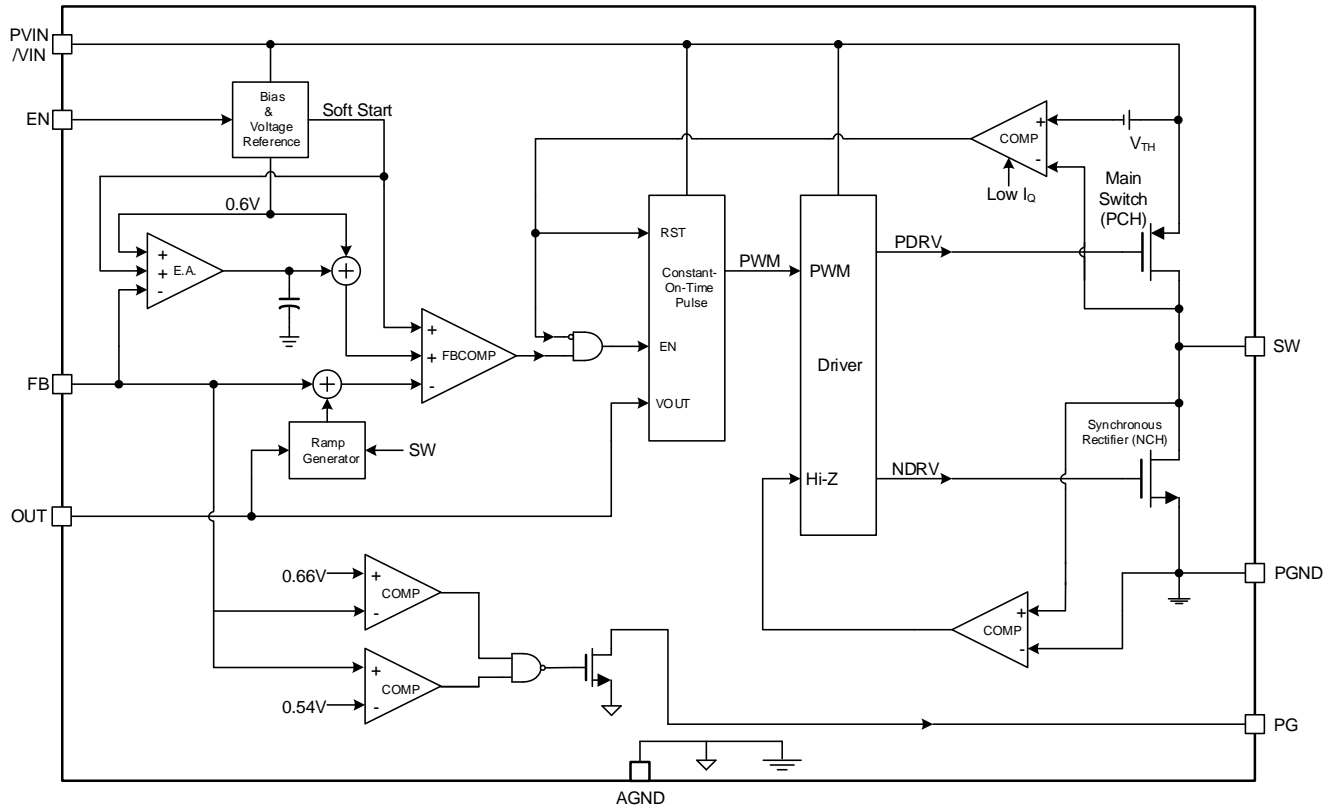
$I_{OUT} = 0A$



**SCP Recovery**

$I_{OUT} = 0A$



**FUNCTIONAL BLOCK DIAGRAM**

**Figure 1: Functional Block Diagram**

## OPERATION

The MP2174C uses constant-on-time control with input voltage feed forward to stabilize the switching frequency over the full input range.

### Constant-On-Time Control

Compare to fixed-frequency PWM control, constant-on-time control offers the advantage of a simpler control loop and faster transient response. By using input voltage feed forward, the MP2174C maintains a nearly constant switching frequency across the input and output voltage ranges. The on-time of the switching pulse can be estimated with Equation (1):

$$t_{ON} = \frac{V_{OUT}}{V_{IN}} \cdot 0.909\mu s \quad (1)$$

To prevent inductor current runaway during load transient, the MP2174C limits the minimum off time to 100ns. This minimum off time limit does not affect the operation of the MP2174C in steady state in any way.

### Forced PWM Operation

The MP2174C works in continuous conduction mode (CCM) to achieve a smaller  $V_O$  ripple, load regulation, and load transient across the full load range.

### Enable

When the input voltage exceeds the under-voltage lockout (UVLO) threshold (typically 2.5V), the MP2174C can be enabled by pulling the EN pin above 0.65V (typical). Leaving EN below 0.55V (typical) or floating it disables the MP2174C. There is an internal 1M $\Omega$  resistor from the EN pin to ground.

When EN is pulled down, there is a discharge path for output. All processes, from EN turning off to the output dropping to 0V, take less than 0.8ms.

### Soft Start/Stop

The MP2174C has a built-in soft start that ramps up the output voltage in a controlled slew rate, avoiding overshoot at start-up. The soft-start time is typically about 0.5ms.

When disabled, the MP2174C ramps down the internal reference and allows the load to linearly discharge the output. The soft-stop time is less than 0.3ms.

### Power Good Indicator

The MP2174C has an open-drain output. The PG pin requires an external pull-up resistor (100k $\Omega$  to 500k $\Omega$ ) for the power good indicator.

When the FB pin is within  $\pm 10\%$  of the regulation voltage (i.e. 0.6V), the PG pin is pulled up. If the FB voltage is out of the  $\pm 10\%$  window, PG is pulled down to ground by an internal MOSFET. The MOSFET has a maximum  $R_{DS(ON)}$  of less than 100 $\Omega$ .

### Current Limit

The MP2174C has a typical 6.5A current limit for the HS-FET, and a 4.5A current limit for the LS-FET. Once the high-side switch hits current limit, the MP2174C turns off the HS-FET and turns on the LS-FET to reduce the inductor current. When the inductor current drops to the valley current limit, the LS-FET turns off and the HS-FET turns on. If the HS-FET reaches the peak current limit and the LS-FET reaches the valley current limit every cycle for 150 $\mu s$ , the MP2174C remains in hiccup mode until the current decreases. This prevents the inductor current from continuing to build up, which could result in damage to the components.

### Short Circuit and Recovery

If the output voltage of the buck converter is shorted to GND, the current limit is triggered. If the current limit is triggered every cycle for 150 $\mu s$ , the MP2174C enters hiccup mode. It disables the output power stage, discharges the soft-start capacitor, and then automatically retries soft start. If the short-circuit condition still remains after soft start ends, the MP2174C repeats this operation cycle until the short condition is removed and the output rises back to the regulation level.

## APPLICATION INFORMATION

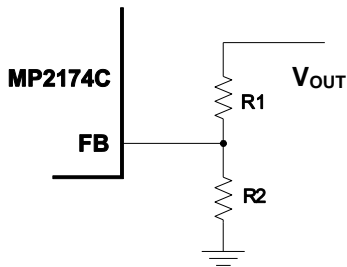
### COMPONENT SELECTION

#### Setting the Output Voltage

The external resistor divider is used to set the output voltage (see the Typical Application Circuit section on page 15). Choose a larger resistance for lower leakage or a smaller one to avoid noise. Choose R1 to be between 120kΩ and 200kΩ. R2 is then calculated using Equation (2):

$$R2 = \frac{R1}{\frac{V_{OUT}}{0.6} - 1} \quad (2)$$

Figure 2 shows the feedback circuit.



**Figure 2: Feedback Network**

Table 1 lists the recommended resistor values for common output voltages.

**Table 1: Resistor Selection for Common Output Voltages**

V <sub>OUT</sub> (V)	R1 (kΩ)	R2 (kΩ)
1.0	200 (1%)	300 (1%)
1.2	200 (1%)	200 (1%)
1.8	200 (1%)	100 (1%)
2.5	200 (1%)	63.2 (1%)
3.3	200 (1%)	44.2 (1%)

#### Selecting the Inductor

A 0.82μH to 4.7μH inductor is recommended for most applications. For highest efficiency, the inductor DC resistance should be small. For most designs, the inductance value can be determined with Equation (3):

$$L_1 = \frac{V_{OUT} \times (V_{IN} - V_{OUT})}{V_{IN} \times \Delta I_L \times f_{OSC}} \quad (3)$$

Where  $\Delta I_L$  is the inductor ripple current.

Choose the inductor current to be approximately 30% of the maximum load current. Calculated the maximum inductor peak current with Equation (4):

$$I_{L(MAX)} = I_{LOAD} + \frac{\Delta I_L}{2} \quad (4)$$

#### Selecting the Input Capacitor

The step-down converter has a discontinuous input current, and a capacitor is required to supply the AC current to the converter while maintaining the DC input voltage. Use low-ESR capacitors for the best performance. Ceramic capacitors with X5R or X7R dielectrics are highly recommended because of their low ESR and small temperature coefficients. For most applications, a 10μF capacitor is sufficient. For a higher output voltage, a 47μF capacitor may be needed to stabilize the system.

Since the input capacitor absorbs the input switching current, it requires an adequate ripple current rating. The RMS current in the input capacitor can be estimated with Equation (5):

$$I_{C1} = I_{LOAD} \times \sqrt{\frac{V_{OUT}}{V_{IN}} \times \left(1 - \frac{V_{OUT}}{V_{IN}}\right)} \quad (5)$$

The worst-case condition occurs at  $V_{IN} = 2V_{OUT}$ , calculated with Equation (6):

$$I_{C1} = \frac{I_{LOAD}}{2} \quad (6)$$

For simplification, choose an input capacitor with an RMS current rating greater than half of the maximum load current.

The input capacitor can be electrolytic, tantalum, or ceramic. When using electrolytic or tantalum capacitors, place a small, high-quality ceramic capacitor (e.g. 0.1μF) as close to the IC as possible. When using ceramic capacitors, ensure that they have enough capacitance to provide sufficient charge to prevent excessive voltage ripple at the input. The input voltage ripple caused by the capacitance can be estimated with Equation (7):

$$\Delta V_{IN} = \frac{I_{LOAD}}{f_{SW} \times C1} \times \frac{V_{OUT}}{V_{IN}} \times \left(1 - \frac{V_{OUT}}{V_{IN}}\right) \quad (7)$$

### Selecting the Output Capacitor

An output capacitor (C2) is required to maintain the DC output voltage.

Low-ESR ceramic capacitors can be used with the MP2174C to keep the output ripple low. Generally, a 10µF output ceramic capacitor is sufficient. In higher output voltage conditions, a 22µF capacitor may be needed for system stability.

Using ceramic capacitors, the capacitance dominates the impedance at the switching frequency, and is the main cause of the output voltage ripple. For simplification, the output voltage ripple can be estimated with Equation (8):

$$\Delta V_{OUT} = \frac{V_{OUT}}{8 \times f_{SW}^2 \times L_1 \times C2} \times \left( 1 - \frac{V_{OUT}}{V_{IN}} \right) \quad (8)$$

For tantalum or electrolytic capacitors, the ESR dominates the impedance at the switching frequency. For simplification, the output ripple can be estimated with Equation (9):

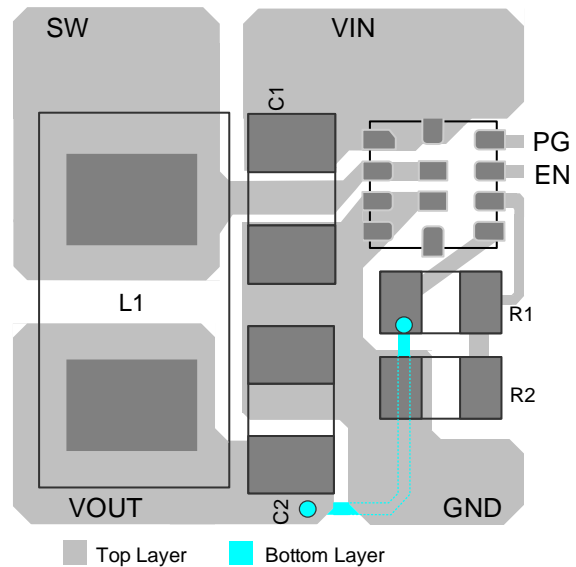
$$\Delta V_{OUT} = \frac{V_{OUT}}{f_{SW} \times L_1} \times \left( 1 - \frac{V_{OUT}}{V_{IN}} \right) \times R_{ESR} \quad (9)$$

The characteristics of the output capacitor also affect the stability of the regulation system.

### PCB Layout Guidelines

Efficient PCB layout is critical for stable operation. For best results, refer to Figure 3 and follow the guidelines below:

1. Place the input decoupling capacitor as close as possible to the IC pins, pin 1 and pin 3 (an 0805 ceramic capacitor is used).
2. Ensure the two ends of the ceramic capacitor are connected directly to PVIN (pin 1) and PGND (pin 3).



**Figure 3: Recommended PCB Layout**

### TYPICAL APPLICATION CIRCUIT

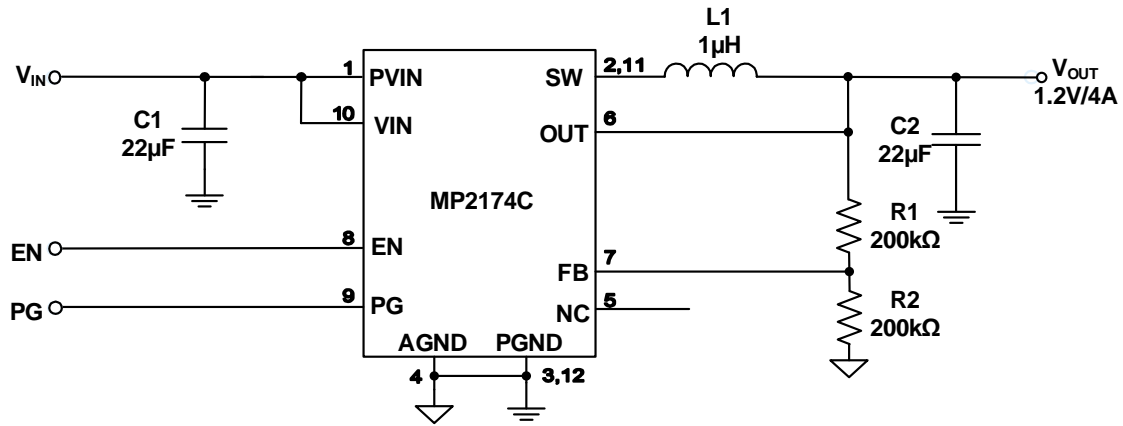


Figure 4: 5V<sub>IN</sub>, 1.2 V/4A